Signal-Carrier Cooperative DF Relay Using Adaptive Modulation

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SUMMARY 2-time slot cooperative relay can be used to increase the cell-edge throughput. Adaptive data modulation further improves the throughput. In this paper, we introduce adaptive modulation to single-carrier (SC) cooperative decode-and-forward (DF) relay. The best modulation combination for mobile-terminal (MT)-relay station (RS) and RS-base station (BS) links is determined for the given local average signal-to-noise power ratios (SNRs) of MT-BS, MT-RS and RS-BS links. According to the modulation combination, the ratio of time slot length of the MT-RS link (first time slot) and the RS-BS link (second time slot) is changed. It is shown by computer simulation that the use of adaptive modulation can achieve higher throughput than fixed modulation and reduces by about 9 dB the required normalized total transmit SNR for a 10%-outage throughput of 0.8 bps/Hz compared to direct transmission.

key words: cooperative decode-and-forward (DF) relay, single-carrier transmission, adaptive modulation

1. Introduction

In the next generation mobile communication systems, broadband data transmissions are required. Since the uplink communication range is limited in general by the mobile terminal (MT) transmit power, the signal waveform having low peak-to-average power ratio (PAPR) property is desirable. 2-time slot cooperative relay [2], [3] is a well-known technique to extend the uplink communication range. In the first time slot, MT transmits its signal to both a relay station (RS) and a base station (BS). Then, in the second time slot, RS forwards its received signal to BS. BS combines the two signals received in the first and second time slot. There are two types of relay protocol: amplify-and-forward (AF) relay protocol and decode-and-forward (DF) relay protocol [3]. In this paper, the DF relay protocol is considered.

In broadband data transmissions, the channel becomes severely frequency-selective and strong inter-symbol interference (ISI) is produced, thereby the degrading the transmit performance [4]. Orthogonal frequency division multiplexing (OFDM) can cope with the severe channel frequency-selectivity and achieves a good transmission performance. However, OFDM has a drawback of high PAPR. For uplink transmissions, single carrier (SC) transmission is promising due to its lower PAPR property than OFDM. The use of minimum mean square error based frequency-domain equalization (MMSE-FDE) in SC transmission can take advantage of the channel frequency-selectivity and achieves a good transmission performance [5]. Therefore, we have been paying attention to SC cooperative relay.

The throughput achievable by the cooperative DF relay depends on link of MT-BS, MT-RS, and RS-BS. However, the relay approach is most effective when the MT-RS direct link quality is poor (i.e., when an MT is close to the cell-edge). Therefore, the throughput gain of cooperative relay can be upper-limited by the worse link between the MT-RS link and the RS-BS link [3]. The MT-RS link quality may change over time according to the movement of MT. RS must forward the same amount of data in the second time slot (RS-BS link transmission) as that received in the first time slot (MT-RS link transmission). DF protocol can provide better throughput than AF protocol by adapting data modulation (accordingly, by adapting the ratio of first and second time slot lengths) to match the changing condition of two links. Fiding the optimum modulation combination is an important issue in 2-time slot cooperative DF relay.

There have been many studies on adaptive modulation for cooperative DF relay [6]–[10]. In [6], the cooperative diversity with 2-time slot incremental relay using adaptive modulation scheme was proposed. The modulation combination is selected according to a predetermined threshold of channel quality. In [7], the bit error rate (BER)-based selection combining was proposed; the modulation combination is selected that minimizes the BER after the selections combining at BS. In [8], the adaptive modulation for the demodulation-and-forward relay protocol instead of DF relay was proposed, where RS demodulates/re-modulates the received signal without data decision and the selection combining is used at RS. The modulation combination which satisfies the BER requirement at BS is selected. Refs. [9], [10] proposed adaptive modulation for opportunistic DF relay, where adaptive modulation is jointly performed with relay selection. However, in [6]–[10], a frequency-nonselective fading is assumed and therefore, no equalization technique is considered. Furthermore, Refs. [6]–[10] assume the selection combining at BS.

In this paper, we introduce adaptive modulation to 2-time slot uplink SC cooperative DF relay using MMSE-FDE in a frequency-selective fading channel. We consider two diversity combining schemes: MMSE-FDE combining and log-likelihood ratio (LLR) combining, to obtain higher spatial diversity gain than the selection combining. Further-
more, noting that in broadband SC, the instantaneous signal-to-noise power ratio (SNR) approaches the local average received SNR, the modulation selection is determined based on the local average SNRs of MT-BS, MT-RS, and RS-BS links. According to the modulation combination, the ratio of time slot lengths of the MT-RS link (first time slot) and the RS-BS link (second time slot) is changed.

The rest of this paper is organized as follows. Sect. 2 presents 2-time slot uplink SC cooperative DF relay with adaptive modulation. In Sect. 3, MMSE-FDE at RS and signal combining at BS are described. The computer simulation results are discussed in Sect. 4. Sect. 5 concludes this paper.

2. Cooperative DF Relay with Adaptive Modulation

2.1 Network Model

In this paper, we consider the uplink SC cooperative DF relay with adaptive modulation. Figure 1 illustrates the cooperative DF relay network model. For simplicity, the single-layer with adaptive modulation. Figure 1 illustrates the cooperation results are discussed in Sect. 4. Sect. 5 concludes this paper. We assume that each of channels of MT-BS, MT-RS, and RS-BS links is characterized by the propagation path loss, the shadowing loss, and the symbol spaced L-path frequency-selective fading. The total transmit power \( P \) is assumed to be equally allocated between MT and RS, i.e., \( P_M = P_R = P/2 \), where \( P_M \) and \( P_R \) are the transmit power at MT and RS, respectively. The RS selection is based on the instantaneous SNR of the worst link between MT-RS and RS-BS. The RS selection is expressed as

\[
R = \arg\max_{R' \in \{0, 1, \ldots, X - 1\}} \left\{ \min_{\alpha} \left( \sum_{l=0}^{L-1} |h_{l_{M-R}}^{(\alpha)}|^2 r_{M-R}^{-\alpha} 10^{-2\eta_{l_{M-R}}}, \sum_{l=0}^{L-1} |h_{l_{B-R}}^{(\alpha)}|^2 r_{B-R}^{-\alpha} 10^{-2\eta_{l_{B-R}}}, \right) \right\},
\]

where \( \alpha \) denotes the path loss exponent, \( \eta_{l_{M-R}} \) and \( \eta_{l_{B-R}} \) are the independent log-normally distributed shadowing losses with standard deviation \( \sigma \) in dB for the MT-RS and RS-BS links, respectively, and \( h_{l_{M-R}}^{(\alpha)} \) and \( h_{l_{B-R}}^{(\alpha)} \) are the complex-valued Lth path gains of MT-RS and RS-BS links, respectively, with \( E \left[ \sum_{l=0}^{L-1} |h_{l_{M-R}}^{(\alpha)}|^2 \right] = 1 \) and \( E \left[ \sum_{l=0}^{L-1} |h_{l_{B-R}}^{(\alpha)}|^2 \right] = 1 \).

2.2 Adaptive Modulation

In this paper, the perfect knowledge of channel state information (CSI) of the MT-BS, MT-RS, and RS-BS links is assumed to be available at BS. The best modulation combination is predetermined for each set of the MT-BS, MT-RS, and RS-BS link CSIs and is stored in a look-up-table at BS. Then, BS informs both MT and RS the modulation to use.

In this paper, the best modulation combination to be stored in the look-up-table at BS will be found by the preliminary computer simulation (see Sect. 4.1).

Figure 2 shows the 2-time slot cooperative DF relay protocol. The first and second time slots constitute a frame of constant number of symbols. The frame length in symbols is denoted by \( K \). The modulation levels may not necessarily be the same for the first and second time slots. Denoting the modulation level and number of symbols in the first (second) time slot by \( m_1 \) (\( m_2 \)) and \( K_1 \) (\( K_2 \)), respectively, we have

\[
\begin{align*}
    m_1 K_1 &= m_2 K_2 \\
    K_1 + K_2 &= K
\end{align*}
\]

An example of modulation combination for the case of \( K = 768 \) symbols/frame is shown in Fig. 3.

The amount of data bits per frame which can be transferred from MT to BS is given by \( K m_1 m_2 / (m_1 + m_2) \) from Eq. (2). Assuming the selective repeat automatic repeat request (SR-ARQ), the throughput \( S \) is defined as

\[
S = \frac{1}{1 + N_g / N_c} \frac{m_1 m_2}{m_1 + m_2} [1 - \text{PER}(m_1, m_2)] \text{ (bps/Hz)},
\]

where \( N_g \) and \( N_c \) are the number of guard interval and channel symbols, respectively, and \( \text{PER}(m_1, m_2) \) is the probability of error.

![Fig. 1 Relay network model.](Image 178x284 to 194x284)

![Fig. 2 Uplink cooperative DF relay protocol.](Image 335x56 to 373x56)

![Fig. 3 A typical example of modulation combination for K = 768 symbols/frame.](Image 375x56 to 405x56)
where $PER(m_1, m_2)$ denotes the packet error rate. $N_r$ and $N_g$ are the Fast Fourier transform (FFT) block size and the cyclic prefix (CP) length, respectively. The modulation combination is selected which maximizes $S$ for the given MT-BS, MT-RS, and RS-BS links.

3. MMSE-FDE at RS and Signal Combining at BS

Since the modulation levels used in the first and second time slot may not be necessarily the same, an important issue is how to combine the signal received directly from MT (first time slot) and the one received via RS (second time slot). In this section, we present the signal combining method at BS.

Below, the symbol-spaced discrete-time signal representation is used.

3.1 Single-Carrier Transmission

During the first time slot, the data-modulated symbol sequence is divided into a sequence of $N_c$ symbol blocks. The last $N_g$ symbols of each $N_c$ symbol block are inserted into the guard interval (GI) as CP. Then, MT broadcasts the sequence of CP-inserted symbol blocks to both RS and BS. RS applies MMSE-FDE to each CP-removed $N_c$ symbol block and carries out the block data detection. During the second time slot, RS re-modulates the recovered data block and transmits it to BS after CP insertion. BS combines the signal blocks received from MT in the first time slot and RS in the second time slot.

The CP-removed received signal blocks at RS and BS in the first time slot are respectively denoted by $\{y_{Mt-R}(t); t=0, \ldots, N_c-1\}$ and $\{y_{Mt-B}(t); t=0, \ldots, N_c-1\}$. They can be expressed as

$\begin{align*}
\hat{y}_{Mt-R}(t) &= \sqrt{2P_{Mt-R}} \sum_{l=0}^{L-1} h_{Mt-R}^{l}(t) s_{M}(t-l) \mod N_c \\
&+ n_{Mt-R}(t), \\
\hat{y}_{Mt-B}(t) &= 2P_{Mt-B} \sum_{l=0}^{L-1} h_{Mt-B}^{l}(t) \mod N_c \\
&+ n_{Mt-B}(t),
\end{align*}$

(4)

where $\{s_{M}(t); t=0, \ldots, N_c-1\}$ is the transmitted symbol block from MT. $h_{Mt-R}^{l}(t)$ is the complex-valued path gain of MT-BS link with $E \left[ \sum_{l=0}^{L-1} h_{Mt-R}^{l}(t)^2 \right] = 1$. $\tau_{Mt-R}^{l}$ and $\tau_{Mt-B}^{l}$ are the time delays of the $l$-th path of the links between MT and RS and between MT and BS, respectively. $n_{Mt-R}(t)$ and $n_{Mt-B}(t)$ are the zero-mean complex-valued noise samples with variance $2\sigma_n^2 = 2N_0/T_s$, where $T_s$ is the symbol duration and $N_0$ is the single-sided power spectral density of the additive white Gaussian noise (AWGN). $P_{Mt-R}$ and $P_{Mt-B}$ are the local average received signal powers for the MT-BS and MT-RS links, respectively. They are given as

$\begin{align*}
P_{Mt-R} &= P_M \cdot D^{-\alpha} \\
P_{Mt-B} &= P_M \cdot D^{-\alpha},
\end{align*}$

(5)

where $P_M = P_M \cdot D^{-\alpha}$ is the normalized transmit power at MT with $\tilde{r}_{Mt-R} = r_{Mt-R}/D$ and $\tilde{r}_{Mt-B} = r_{Mt-B}/D$ being the normalized distances between MT and RS and between MT and BS, respectively. $\eta_{Mt-R}$ is the independent log-normally distributed shadowing loss with standard deviation $\sigma$ in dB for the MT-BS.

The CP-removed received signal blocks at BS in the second time slot is denoted by $\{y_{Mt-B}(t); t=0, \ldots, N_c-1\}$. $y_{Mt-B}(t)$ can be expressed as

$y_{Mt-B}(t) = 2P_{Mt-B} \sum_{l=0}^{L-1} h_{Mt-B}^{l}(t) \mod N_c + n_{Mt-B}(t),

(6)$

where $\{s_{M}(t); t=0, \ldots, N_c-1\}$ is the transmitted symbol block from RS. $\tau_{Mt-B}^{l}$ is the time delay of the RS-BS link. $n_{Mt-B}(t)$ is the Gaussian noise with zero mean and variance $2N_0/T_s$ at BS during the second time slot. $P_{Mt-B}$ is the local average received signal power for the RS-BS link and is given as

$P_{Mt-B} = P_R \cdot D^{-\alpha} \cdot 10^{-\eta_{Mt-B}/10},

(7)$

where $P_R = P_R \cdot D^{-\alpha}$ is the normalized transmit power at RS, $\tilde{r}_{Mt-B} = r_{Mt-B}/D$ is the normalized distance between RS and BS.

3.2 FDE at RS

Figure 4 illustrates the RS transceiver structure. The CP-removed received signal block $\{y_{Mt-R}(t); t=0, \ldots, N_c-1\}$ is transformed by $N_c$-point fast Fourier transform (FFT) to the frequency-domain received signal $\{Y_{Mt-R}(k); k=0, \ldots, N_c-1\}$. $Y_{Mt-R}(k)$ is given as

$Y_{Mt-R}(k) = \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} y_{Mt-R}(t) \exp \left( -j2\pi k t / N_c \right),

(8)$

where

$S_{M}(k) = \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} s_{M}(t) \exp \left( -j2\pi k t / N_c \right),

H_{Mt-R}(k) = \sqrt{2P_{Mt-R}} \sum_{l=0}^{L-1} h_{Mt-R}^{l}(t) \exp \left( -j2\pi k \tilde{r}_{Mt-R}^{l} / N_c \right),

\Pi_{Mt-R}(k) = \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} n_{Mt-R}(t) \exp \left( -j2\pi k t / N_c \right).

(9)$

Then, one-tap MMSE-FDE is applied as

$\hat{Y}_{Mt-R}(k) = Y_{Mt-R}(k)W_{Mt-R}(k),

(10)$

where $W_{Mt-R}(k)$ is the MMSE-FDE weight (which minimizes the mean square error (MSE) between $\hat{Y}_{Mt-R}(k)$ and

Fig. 4 RS structure.
where \( (\cdot)^* \) denotes the complex conjugate operation.

The frequency-domain signal \( \{\hat{y}_{M-\eta}(k); k=0, \ldots, N_c-1\} \) after MMSE-FDE is transformed by \( N_c \)-point inverse FFT (IFFT) back to the time-domain signal block \( \{d_{M-\eta}(t); t=0, \ldots, N_c-1\} \). \( d_{M-\eta}(t) \) is given as

\[
\hat{d}_{M-\eta}(t) = \frac{1}{\sqrt{N_c}} \sum_{k=0}^{N_c-1} \hat{y}_{M-\eta}(k) \exp \left( j2\pi \frac{k}{N_c} t \right)
\]

\[
= \frac{1}{\sqrt{N_c}} \sum_{k=0}^{N_c-1} H_{M-\eta}(k) W_{M-\eta}(k) s_M(t) \exp \left( j2\pi \frac{k}{N_c} t \right) + \frac{1}{\sqrt{N_c}} \sum_{k=0}^{N_c-1} H_{M-\eta}(k) \Pi_{M-\eta}(k) \exp \left( j2\pi \frac{k}{N_c} t \right)
\]

(12)

where the first term is the desired signal and the second and third terms are respectively the residual inter-symbol interference (ISI) and the noise.

Finally, the data decision and data re-modulation is done to generate the symbol block \( \{s_R(t); t=0, \ldots, N_c-1\} \), which is to be relayed to BS in the second time slot. In this paper, we consider the fixed DF relay protocol [3], in which RS transmits the re-modulated signal to BS in the second time slot even if data errors exist after decoding at RS.

### 3.3 Signal Combining at BS

Figure 5 illustrates the BS receiver structure. \( N_c \)-point FFT is applied to \( \{y_{M-\eta}(t); t=0, \ldots, N_c-1\} \) and \( \{y_{R-\eta}(t); t=0, \ldots, N_c-1\} \) to transform them into the frequency-domain received signals, \( \{Y_{M-\eta}(k); k=0, \ldots, N_c-1\} \) and \( \{Y_{R-\eta}(k); k=0, \ldots, N_c-1\} \), respectively. \( Y_{M-\eta}(k) \) and \( Y_{R-\eta}(k) \) are given as

\[
\begin{align*}
Y_{M-\eta}(k) &= \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} y_{M-\eta}(t) \exp \left( -j2\pi \frac{k}{N_c} t \right) \\
&= H_{M-\eta}(k) S_M(k) + \Pi_{M-\eta}(k) \\

Y_{R-\eta}(k) &= \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} y_{R-\eta}(t) \exp \left( -j2\pi \frac{k}{N_c} t \right) \\
&= H_{R-\eta}(k) S_R(k) + \Pi_{R-\eta}(k)
\end{align*}
\]

(13)

where

\[
\begin{align*}
S_R(k) &= \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} s_R(t) \exp \left( -j2\pi \frac{k}{N_c} t \right) \\
H_{M-\eta}(k) &= \sqrt{2} |H_{M-\eta}(k)| \sum_{t=0}^{N_c-1} h_{M-\eta}^{(t)}(k) \exp \left( -j2\pi \frac{k}{N_c} t \right) \\
H_{R-\eta}(k) &= \sqrt{2} |H_{R-\eta}(k)| \sum_{t=0}^{N_c-1} h_{R-\eta}^{(t)}(k) \exp \left( -j2\pi \frac{k}{N_c} t \right) \\
\Pi_{M-\eta}(k) &= \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} n_{M-\eta}(t) \exp \left( -j2\pi \frac{k}{N_c} t \right) \\
\Pi_{R-\eta}(k) &= \frac{1}{\sqrt{N_c}} \sum_{t=0}^{N_c-1} n_{R-\eta}(t) \exp \left( -j2\pi \frac{k}{N_c} t \right)
\end{align*}
\]

(14)

(a) In case of same modulation level

If the same data modulation level is used for both the first and second time slots, joint MMSE-FDE combining [5] is applied. The frequency-domain signal \( \{\hat{Y}(k); k=0, \ldots, N_c-1\} \) after joint MMSE-FDE combining is given as

\[
\hat{Y}(k) = Y_{M-\eta}(k) W_{M-\eta}(k) + Y_{R-\eta}(k) W_{R-\eta}(k),
\]

(15)

where \( W_{M-\eta}(k) \) and \( W_{R-\eta}(k) \) are the MMSE weights which jointly minimizes the MSE between \( \hat{Y}(k) \) and \( S_M(k) \) and can be derived from [5] as

\[
\begin{align*}
W_{M-\eta}(k) &= \frac{H_{M-\eta}^*(k)}{|H_{M-\eta}(k)|^2 + \left| H_{R-\eta}(k) \right|^2 + 2\sigma_n^2} \\
W_{R-\eta}(k) &= \frac{H_{R-\eta}^*(k)}{|H_{R-\eta}(k)|^2 + \left| H_{M-\eta}(k) \right|^2 + 2\sigma_n^2}
\end{align*}
\]

(16)

The frequency-domain signal \( \{\hat{Y}(k); k=0, \ldots, N_c-1\} \) is transformed by \( N_c \)-point IFFT back to the time-domain signal \( \{\hat{d}(t); t=0, \ldots, N_c-1\} \) as

\[
\hat{d}(t) = \frac{1}{\sqrt{N_c}} \sum_{k=0}^{N_c-1} \hat{Y}(k) \exp \left( j2\pi \frac{k}{N_c} t \right).
\]

(17)

(b) In case of different modulation levels

If the data modulation level is different in the first and second time slots, the received signals from MT and RS are combined using log-likelihood ratio (LLR) combining [11] after MMSE-FDE. One-tap MMSE-FDE for \( \{Y_{M-\eta}(k); k=0, \ldots, N_c-1\} \) and \( \{Y_{R-\eta}(k); k=0, \ldots, N_c-1\} \) are given as

\[
\begin{align*}
\hat{Y}_{M-\eta}(k) &= Y_{M-\eta}(k) W_{M-\eta}(k) \\
\hat{Y}_{R-\eta}(k) &= Y_{R-\eta}(k) W_{R-\eta}(k)
\end{align*}
\]

(18)

where \( W_{M-\eta}(k) \) and \( W_{R-\eta}(k) \) are the MMSE weights derived from [5] as

\[
\begin{align*}
W_{M-\eta}(k) &= \frac{H_{M-\eta}^*(k)}{|H_{M-\eta}(k)|^2 + 2\sigma_n^2} \\
W_{R-\eta}(k) &= \frac{H_{R-\eta}^*(k)}{|H_{R-\eta}(k)|^2 + 2\sigma_n^2}
\end{align*}
\]

(19)
The frequency-domain signals \( \{ \hat{Y}_{M-R}(k); k = 0, \ldots, N_c - 1 \} \) and \( \{ \hat{Y}_{R-R}(k); k = 0, \ldots, N_c - 1 \} \) after MMSE-FDE are transformed by \( N_c \)-point IFFT back to the time-domain signals \( \{ \hat{d}_{M-R}(t); t = 0, \ldots, N_c - 1 \} \) and \( \{ \hat{d}_{R-R}(t); t = 0, \ldots, N_c - 1 \} \) as

\[
\begin{align*}
\hat{d}_{M-R}(t) &= \frac{1}{\sqrt{N_c}} \sum_{k=0}^{N_c-1} \hat{Y}_{M-R}(k) \exp \left( j \frac{2\pi t k}{N_c} \right) , \\
\hat{d}_{R-R}(t) &= \frac{1}{\sqrt{N_c}} \sum_{k=0}^{N_c-1} \hat{Y}_{R-R}(k) \exp \left( j \frac{2\pi t k}{N_c} \right) ,
\end{align*}
\]

from which the bit-LLRs, \( \lambda_{M-R,x_i}(t) \) and \( \lambda_{R-R,x_i}(t) \) of \( x \)-th bit within \( t \)-th symbol, are computed using [11]

\[
\begin{align*}
\lambda_{M-R,x_i}(t) &= \left( \frac{\hat{d}_{M-R}(t) - \frac{1}{N_c} \sum_{k=0}^{N_c-1} \hat{H}_{M-R}(k) d_{M-R,b(i)=0}}{\sqrt{\hat{\sigma}^2_{M-R}}(t)} \right)^2 , \\
\lambda_{R-R,x_i}(t) &= \left( \frac{\hat{d}_{R-R}(t) - \frac{1}{N_c} \sum_{k=0}^{N_c-1} \hat{H}_{R-R}(k) d_{R-R,b(i)=0}}{\sqrt{\hat{\sigma}^2_{R-R}}(t)} \right)^2 ,
\end{align*}
\]

where

\[
\hat{H}_{M-R}(k) = H_{M-R}(k) W_{M-R}(k) ,
\hat{H}_{R-R}(k) = H_{R-R}(k) W_{R-R}(k) .
\]

In Eq. (21), \( d_{M-R,b(i)=0} \) and \( d_{R-R,b(i)=0} \) are the symbol candidates which have the maximum LLRs within the set of the data symbols. \( 2\sigma^2_{M-R} \) and \( 2\sigma^2_{R-R} \) are the sum variances of the residual ISI and the noise given as

\[
\begin{align*}
2\sigma^2_{M-R} &= \frac{1}{N_c} \sum_{k=0}^{N_c-1} |\hat{H}_{M-R}(k)|^2 \left( \frac{1}{N_c} \sum_{k=0}^{N_c-1} |\hat{H}_{M-R}(k)|^2 \right) , \\
2\sigma^2_{R-R} &= \frac{1}{N_c} \sum_{k=0}^{N_c-1} |\hat{H}_{R-R}(k)|^2 \left( \frac{1}{N_c} \sum_{k=0}^{N_c-1} |\hat{H}_{R-R}(k)|^2 \right) .
\end{align*}
\]

The LLR combining to obtain the LLR \( \lambda_x \) for \( x \)-th bit is given as

\[
\lambda_x = \lambda_{M-R,x_i}(t_1) + \lambda_{R-R,x_i}(t_2) ,
\]

where \( \lambda_{M-R,x_i}(t_1) \) is the LLR of the \( x \)-th bit of the \( t_1 \)-th symbol in the time-domain signal received from MT and \( \lambda_{R-R,x_i}(t_2) \) is the LLR of the \( x \)-th bit of the \( t_2 \)-th symbol in the time-domain signal received from RS. Note that the following relationship between \( \lambda_x \), \( \lambda_{M-R,x_i}(t_1) \) and \( \lambda_{R-R,x_i}(t_2) \) holds:

\[
x = x_1 + m_1 t_1 = x_2 + m_2 t_2 ,
\]

In Eq. (24), if \( \lambda_x \) is positive (negative), the \( x \)-th transmit bit is determined as 1 (0).

### 4. Computer Simulation

The simulation condition is shown in Table 1. We want to discuss the behavior of the adaptive modulation. In the computer simulation, we consider 3 modulation modes, BPSK, QPSK, and 16QAM only and the uncoded transmission. Therefore, there exist nine possible modulation combinations shown in Table 2. A frequency-selective block Rayleigh fading channel having a symbol-spaced L=16-path uniform power delay profile is assumed. In this paper, we assume that the frame length is kept constant, but the ratio of first and second time slot lengths is changed according to the modulation levels used in the first and second time slots. The frame length is kept constant irrespective of the modulation combination. Therefore, the frame length should be a common multiple of block size \( N_c \) and the first time slot to frame length ratio \( m_1 / (m_1 + m_2) \). In the computer simulation, we assume \( N_c=256 \) and consider BPSK, QPSK, and 16QAM data modulation (i.e., \( m_1 / (m_1 + m_2)=2, 3, 4, \) and 5). Therefore, the frame length is set to 30720 symbols, which is the least common multiple of \( N_c=256 \) and \( m_1 / (m_1 + m_2)=2, 3, 4, \) and 5. Figure 6 illustrates the single-cell/single-user relay network model assumed for computer simulation. It is assumed that 6 RSs are located equal-distantly to each other at the normalized distance \( \eta_{R-Q}/D = 0.5 \) from BS. MT location is randomly selected within the cell. The normalized total transmit power \( P = P.B.D^{-\alpha} \) is assumed to be equally allocated to MT and RS as \( P_M = P_R = P/2 \).

### Table 1 Simulation condition.

<table>
<thead>
<tr>
<th>Transmission data</th>
<th>Block size</th>
<th>( N_c = 256 )</th>
<th>CP length</th>
<th>( N_0 = 16 )</th>
</tr>
</thead>
<tbody>
<tr>
<td>Frame size</td>
<td>( K = 30720 )(symbols)</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Channel</td>
<td>Fading type</td>
<td>Block Rayleigh fading</td>
<td>Power delay profile</td>
<td>Uniform</td>
</tr>
<tr>
<td></td>
<td>No. of paths</td>
<td>( L = 16 )</td>
<td>Path loss exponent</td>
<td>( \alpha = 3.5 )</td>
</tr>
<tr>
<td></td>
<td>Shadowing loss standard deviation of MT-RS link</td>
<td>( \sigma = 7.0 )(dB)</td>
<td></td>
<td></td>
</tr>
<tr>
<td>RS Receiver</td>
<td>Equalization</td>
<td>MMSE-FDE</td>
<td>Channel estimation</td>
<td>Ideal</td>
</tr>
<tr>
<td></td>
<td>Equalization</td>
<td>MMSE-FDE</td>
<td>Combining scheme</td>
<td>MMSE-FDE</td>
</tr>
<tr>
<td></td>
<td></td>
<td>combing. LLR combining</td>
<td></td>
<td></td>
</tr>
<tr>
<td></td>
<td>Channel estimation</td>
<td>Ideal</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

### Table 2 Possible modulation combinations.

(Modulation1-Modulation2)

<table>
<thead>
<tr>
<th>BPSK-BPSK</th>
<th>BPSK-QPSK</th>
<th>BPSK-16QAM</th>
</tr>
</thead>
<tbody>
<tr>
<td>QPSK-BPSK</td>
<td>QPSK-QPSK</td>
<td>QPSK-16QAM</td>
</tr>
<tr>
<td>16QAM-BPSK</td>
<td>16QAM-QPSK</td>
<td>16QAM-16QAM</td>
</tr>
</tbody>
</table>
4.1 Finding the Best Modulation Combination

The best modulation combination was found by preliminary computer simulation. Figure 7 illustrates the simulation model. It is assumed that the local average/instantaneous received SNRs of MT-RS and RS-BS links are different by $\Delta_{M\rightarrow R}$ and $\Delta_{R\rightarrow B}$ dB, respectively, from the local average/instantaneous received SNR ($\text{SNR}_{M\rightarrow B}$) of MT-BS link.

Figures 8(a) and (b) show the best modulation combination when the local average received SNR $\text{SNR}_{M\rightarrow B} = 5$ and $10$ dB, respectively. It should be noted that the same amount of data bits must be transmitted in the first and second time slots. It can be seen from Figs. 8(a)(b) that, when the MT-RS link has better channel quality than the RS-BS link, more transmission time is given to the second time slot by using higher modulation level in the first time slot (MT-RS transmission). It can be seen from Fig. 8(a) that when $\Delta_{M\rightarrow R}$ ($\Delta_{R\rightarrow B}$) is high, higher level modulation is used in the first (second) time slot.

For comparison, the best modulation combination found when the instantaneous received SNR $\text{SNR}_{M\rightarrow B} = 5$ and $10$ dB is shown in Figs. 8(c) and (d), respectively. Comparison between Figs. 8(a)(b) and Figs. 8(c)(d) shows that the best modulation combination based on the instantaneous received SNRs differs only slightly from that based on the local average received SNRs. This is because, in a strong frequency-selective fading channel, the instantaneous received SNR varies only slightly and approaches the local average received SNR (see Appendix). Therefore, in the following simulation, the modulation combination found based on the local average received SNR is used.

4.2 Throughput Performance

The average throughput $S$ is computed as
where $p_a$ is the probability that the $a$-th ($a = 0, \ldots, A-1$) modulation combination is selected, $A$ is the number of possible modulation combinations, and $PER_a$, $m_{a,1}$ and $m_{a,2}$ are respectively the PER and the number of bits per symbol in the first and second time slots when the $a$-th modulation combination is used.

Figure 9 plots the 10%-outage throughput (below which the measured throughput falls with the probability of 10%) as a function of the normalized total transmit SNR ($\bar{P}/\sigma_n$) when the shadowing loss of RS-BS link $\eta_{R\rightarrow B} = 0$ dB. For comparison, the 10%-outage throughput of 2-time slot cooperative DF relay using fixed modulation combination is also plotted as the dashed line and that of direct communication using adaptive modulation as the dashed-dotted line. The use of adaptive modulation can achieve higher throughput than fixed modulation. The throughput of direct communication using adaptive modulation is lower than cooperative DF relay using adaptive modulation when the transmit SNR $< 24$ dB. The cooperative DF relay using adaptive modulation reduces by about 9 dB the required SNR for a throughput of 0.8 bps/Hz compared to direct transmission. This is because 10%-outage throughput represents the throughput of a user close to the cell-edge (i.e., the MT-BS link is in a poor condition).

Figure 10 plots the 90%-outage throughput (below which the throughput falls with the probability of 90%) using adaptive modulation when the shadowing loss of RS-BS link $\eta_{R\rightarrow B} = 0$ dB. For comparison, the 90%-outage throughput of cooperative DF relay using fixed modulation combination is also plotted as the dashed lines and that of direct communication using adaptive modulation as the dashed-dotted line. The 90%-outage throughput of direct communication always achieves higher throughput than that of cooperative DF relay using adaptive modulation. This is because 90%-outage throughput represents the throughput of a user close to the center of the cell (i.e., the MT-BS link is in a good condition) and thus, the loss of using 2-time slot relay offsets the spatial diversity gain.

5. Conclusion

In this paper, we introduced the adaptive modulation to 2-time slot uplink SC cooperative DF relay. It was confirmed by computer simulation that cooperative DF relay with adaptive modulation can achieve higher throughput than cooperative DF relay with fixed modulation. However, even if adaptive modulation is used, the throughput of 2-time slot cooperative DF relay degrades compared to direct communication when the MT-BS link is in a good condition (e.g., when MT is close to the center of the cell). Switching between cooperative DF relay and direct communication may always achieve better throughput. This is left as our future work.

Adaptive modulation requires that BS knows the CSIs of MT-BS, MT-RS, and RS-BS links, selects the best modulation combination from the look-up table, and informs the best modulation combination to both MT and RS. How to implement this is an important practical issue and is left as our future study. In the computer simulation, we considered only 3 modulation modes, the uncoded transmission, and equal power allocation. More general adaptive modulation and coding and adaptive power allocation for SC cooperative DF relay are left as our future work.

References

Appendix: Variation of Instantaneous SNR

Assuming a frequency-selective Rayleigh channel and uniform power delay profile, the instantaneous SNR $\gamma_{\text{inst}}$ is given as

$$\gamma_{\text{inst}} = \frac{P_{\text{ave}}}{\sigma_n^2} \sum_{l=0}^{L-1} |h_l|^2 = \gamma_{\text{ave}} \cdot Z,$$  \hspace{1cm} (A·1)

where $\gamma_{\text{ave}} = P_{\text{ave}}/\sigma_n^2$ is the local average received SNR with denoting $P_{\text{ave}}$ and $\sigma_n^2$ as the local average received power and the noise power, respectively. $h_l$ denotes the zero-mean complex valued l-th path gain with $E \left[ \sum_{l=0}^{L-1} |h_l|^2 \right] = 1$, where $E[.]$ denotes the ensemble average operator. In this paper, the uniform power delay profile (i.e., $E \left[ |h_l|^2 \right] = 1/L$) is assumed and hence, the sum of squared path gains, $Z = \sum_{l=0}^{L-1} |h_l|^2$, follows a $\chi^2$-distribution with $2L$ degree-of-freedom. The probability density function (PDF) of $Z$ is given as \cite{12}

$$p(Z) = \frac{L^L}{\Gamma(L)} Z^{L-1} e^{-ZL},$$ \hspace{1cm} (A·2)

where $\Gamma(.)$ denotes the gamma function. The mean $E(Z) = 1$ and the variance $V(Z) = 1/L$. As $L$ increases, $V(Z)$ gets smaller and as a consequence, the instantaneous received SNR approaches the local average received SNR.

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